

DESCRIPTION

RADIO SYSTEM, RADIO TRANSMITTER, AND RADIO RECEIVER

5 Technical Field

[0001] The present invention relates to a radio system,
radio transmission apparatus and radio reception
apparatus, and more particularly, to a radio system, radio
transmission apparatus and radio reception apparatus
10 having an excellent phase noise characteristic.

Background Art

[0002] Conventionally, various measures are adopted to
provide a radio system having an excellent phase noise
15 characteristic. An example of this conventional radio
system having an excellent phase noise characteristic
is described in Patent Document 1. This radio system is
provided with a local noise canceller shown in FIG.14
to improve its phase noise characteristic.

20 [0003] The operation of this local noise canceller will
be explained with reference to FIG.14 and FIG.15. FIG.15
shows characteristic diagrams illustrating frequency
characteristics of the respective components of the local
noise canceller shown in FIG.14.

25 [0004] As shown in FIG.15A, suppose that an input signal
consists of a modulated IF signal (BST-OFDM) multiplexed
with pilot carrier (PILOT) and input phase noise (part

expressed by bold hatching) is superimposed thereon.

[0005] Here, when it is assumed that the frequency of the input pilot carrier is f_{PLT} , frequency of the input signal is f_{sig} and input phase noise is $\theta(t)$, input phase noise $\theta(t)$ is superimposed on f_{PLT} and f_{sig} , and therefore they are expressed as follows:

$$f_{PLT} \angle \theta(t)$$

$$f_{sig} \angle \theta(t)$$

[0006] Input signal A is distributed by distributor 50 and one portion is output to a pilot branch and the other to a signal branch. In the pilot branch, the one signal distributed by distributor 50 is band-limited by band pass filter 51, only a pilot carrier component thereof is allowed to pass and extracted and further subjected to limiter amplification by limiter amplifier 52.

[0007] At this time, the IF signal component is removed from the frequency characteristics of output signal B from band pass filter 51 and output signal C from limiter amplifier 52 as shown in FIG.15B, 15C, and only the pilot carrier component and input phase noise $\theta(t)$ superimposed thereon remain.

[0008] At this time, a delay is produced at band pass filter 51 and if this delay time is assumed to be τ_{BPF1} , input phase noise $\theta(t - \tau_{BPF1})$ delayed by τ_{BPF1} is superimposed on input pilot carrier frequency f_{PLT} , and therefore f_{PLT} is expressed as follows:

$$f_{PLT} \angle \theta(t - \tau_{BPF1})$$

[0009] On the other hand, in the signal branch, local oscillation signal D is output from local oscillator 60. Here, the frequency characteristic of local oscillation signal D output from local oscillator 60 consists of a
5 signal of local oscillation frequency (f_{LO}) and phase noise originating in the system which is superimposed thereon as shown in FIG.15D.

[0010] Here, if it is assumed that the local oscillation signal frequency in the system is f_{LO} and the local
10 oscillation signal phase noise in the system is $\phi(t)$, local oscillation signal phase noise $\phi(t)$ in the system is superimposed on the local oscillation signal frequency f_{LO} in the system, and therefore f_{LO} is expressed as follows:

$$f_{LO} \angle \phi(t)$$

15 [0011] In the signal branch, the frequency of the signal output from distributor 50 is converted by frequency converter 61 using local oscillation signal D from local oscillator 60 and signal E is output.

[0012] Here, the frequency characteristic of signal E
20 output from frequency converter 61 includes a sum component and difference component between input signal A and local oscillation signal D as shown in FIG.15E. Thus, relationships between the respective signal components included in signal E and phase noise to be
25 superimposed thereon are expressed as follows:

$$f_{PLT} - f_{LO} \angle \theta(t) - \phi(t)$$

$$f_{sig} - f_{LO} \angle \theta(t) - \phi(t)$$

$$f_{\text{PLT}} + f_{\text{LO}} \angle \theta(t) + \varphi(t)$$

$$f_{\text{sig}} + f_{\text{LO}} \angle \theta(t) + \varphi(t)$$

[0013] Frequency-converted signal E is band-limited by band pass filter 62 so that only the difference component
 5 passes, and therefore it is output from band pass filter 62 as signal F and the frequency characteristic of signal F is deprived of the sum component in E and only the difference component exists as shown in FIG.15F.

[0014] At this time, a delay is produced at band pass
 10 filter 62 and if this delay time is assumed to be τ_{BPF2} , delay τ_{BPF2} is produced in the phase noise superimposed on the extracted difference component and relationships between the respective signal components included in signal F and phase noise to be superimposed thereon are
 15 expressed as follows:

$$f_{\text{PLT}} - f_{\text{LO}} \angle \theta(t - \tau_{\text{BPF2}}) - \varphi(t - \tau_{\text{BPF2}})$$

$$f_{\text{sig}} - f_{\text{LO}} \angle \theta(t - \tau_{\text{BPF2}}) - \varphi(t - \tau_{\text{BPF2}})$$

[0015] A delay is then added to signal F by delay compensator 63 so as to be equivalent to the delay time
 20 at band pass filter 51 in the pilot branch and the signal with the delay is output as signal G.

[0016] Here, when it is assumed that the delay time of band pass filter 62 with respect to delay time τ_{BPF1} of band pass filter 51 is τ_{BPF2} and the delay time at delay
 25 compensator 63 is Δt , delay compensator 63 adds delay Δt to signal F in such a way that

$$\tau_{\text{BPF1}} = \tau_{\text{BPF2}} + \Delta t$$

to equalize the delay time difference between the signal branch and pilot branch.

[0017] As a result, the frequency characteristic of signal G does not change as shown in FIG.15G and relationships between the respective signal components included in signal G and phase noise to be superimposed thereon consist of phase noise plus delay Δt as follows:

$$f_{PLT} - f_{LO} \angle \theta(t - \tau_{BPF2} - \Delta t) - \phi(t - \tau_{BPF2} - \Delta t)$$

$$f_{sig} - f_{LO} \angle \theta(t - \tau_{BPF2} - \Delta t) - \phi(t - \tau_{BPF2} - \Delta t)$$

10 [0018] Signal G in the signal branch and signal C in the pilot branch output from above described limiter amplifier 52 are frequency-converted by frequency converter 70 and output as signal H.

[0019] Here, the frequency characteristic of signal H output from frequency converter 70 includes the sum component and difference component between signal G and signal C as shown in FIG.15H. Therefore, relationships between the respective signal components included in signal H and phase noise to be superimposed thereon are expressed as follows:

$$f_{PLT} - (f_{PLT} - f_{LO}) \angle \theta(t - \tau_{BPF1}) - \{\theta(t - \tau_{BPF2} - \Delta t) - \phi(t - \tau_{BPF2} - \Delta t)\}$$

$$f_{PLT} - (f_{sig} - f_{LO}) \angle \theta(t - \tau_{BPF1}) - \{\theta(t - \tau_{BPF2} - \Delta t) - \phi(t - \tau_{BPF2} - \Delta t)\}$$

$$f_{PLT} + (f_{PLT} - f_{LO}) \angle \theta(t - \tau_{BPF1}) + \{\theta(t - \tau_{BPF2} - \Delta t) - \phi(t - \tau_{BPF2} - \Delta t)\}$$

$$f_{PLT} + (f_{sig} - f_{LO}) \angle \theta(t - \tau_{BPF1}) + \{\theta(t - \tau_{BPF2} - \Delta t) - \phi(t - \tau_{BPF2} - \Delta t)\}$$

25 [0020] Here, as shown above, delay compensator 63 adds delay Δt in such a way that:

$$\tau_{BPF1} = \tau_{BPF2} + \Delta t$$

to equalize the delay time difference between the signal branch and pilot branch, and therefore the expression can be organized as follows:

$$f_{LO} \angle \varphi(t - \tau_{BPF2} - \Delta t)$$

$$5 \quad f_{LO} - (f_{sig} - f_{PLT}) \angle \varphi(t - \tau_{BPF2} - \Delta t)$$

$$2 \times f_{PLT} - f_{LO} \angle 2 \times \theta(t - \tau_{BPF1}) - \varphi(t - \tau_{BPF2} - \Delta t)$$

$$f_{PLT} + (f_{sig} - f_{LO}) \angle 2 \times \theta(t - \tau_{BPF1}) - \varphi(t - \tau_{BPF2} - \Delta t)$$

[0021] Here, if attention is focused on the difference component, the frequency of the output signal component is frequency (f_{LO}) of the local oscillation signal in the system irrespective of the frequency of the input signal, that is, constant. Furthermore, the side band of the signal when focused on the pilot carrier is reversed between the input and output.

15 [0022] Furthermore, input phase noise $\theta(x)$ is canceled and the phase noise of the output signal becomes phase noise $\varphi(x)$ of the local oscillation signal in the system instead. That is, it is understandable that when phase noise $\varphi(x)$ of the local oscillation signal in the system is small enough, the phase noise of the input signal is sufficiently reduced and output.

[0023] Thus, signal H frequency-converted by frequency converter 70 is band-limited by band pass filter 71 so that only the difference component passes and signal I is output so that only the signal component passes, and the frequency characteristic of signal I is deprived of the sum component in H and the pilot carrier component

in the difference component as shown in FIG.15I, includes only the signal component of the difference component and the relationship between the signal component included in signal I and phase noise to be superimposed thereon is as follows:

$$f_{LO} - (f_{sig} - f_{PLT}) \angle \varphi(t - \tau_{BPF2} - \Delta t)$$

[0024] Based on the principles of frequency synchronization and noise cancellation by the above described local noise canceller, even if a frequency deviation is produced on an input signal, for example, it is possible to obtain an output signal at a frequency following the local oscillation frequency having a high degree of stability with high frequency accuracy generated by local oscillator 60 and thereby eliminate the frequency deviation of the input signal.

[0025] Furthermore, with phase noise $\theta(x)$ superimposed on the input signal canceled, the phase noise of the output signal becomes only phase noise $\varphi(x)$ of the local oscillation signal in the system instead, and therefore if phase noise $\varphi(x)$ of the local oscillation signal in the system is small enough, the phase noise of the input signal is sufficiently reduced and output.

[Patent Document 1] Japanese Patent Application
Laid-Open No.2002-152158

Disclosure of Invention

Problems to be Solved by the Invention

[0026] However, phase noise $\theta(x)$ generated from local oscillator 60 is not canceled in the conventional radio system and phase noise increases at a rate of $20 \cdot \log$ (corresponds to a multiple of the frequency), and therefore when the frequency of local oscillator 60 is high, there is a problem that communication quality deteriorates due to influences of phase noise $\theta(x)$.

[0027] It is an object of the present invention to provide a radio system, radio transmission apparatus and radio reception apparatus that improves the phase noise characteristics and thereby improves communication quality.

15 Means for Solving the Problem

[0028] The radio system of the present invention adopts a configuration comprising a radio transmission apparatus provided with a transmission section that transmits a radio signal which multiplexes a modulated signal without the signal being carried on a center frequency and a pilot signal having a center frequency identical to the center frequency, and a radio reception apparatus provided with an antenna that receives the radio signal, a distribution section that distributes the received signal received by the antenna into two directions, an extraction section that extracts a signal component corresponding to the pilot signal from one signal distributed by the

distribution section and outputs the signal component, a delay addition section that gives a delay to the other signal distributed by the distribution section and outputs the signal, and a quadrature demodulation section that frequency-multiplies the output signal of the extraction section by the output signal of the delay addition section and carries out quadrature demodulation.

[0029] The radio reception apparatus of the present invention adopts a configuration comprising an antenna that receives a radio signal which multiplexes a modulated signal without the signal being carried on a center frequency and a pilot signal having a center frequency identical to the center frequency, a distribution section that distributes the received signal received by the antenna into two directions, an extraction section that extracts a signal component corresponding to the pilot signal having a center frequency identical to the center frequency from one signal distributed by the distribution section, a delay addition section that gives a delay to the other received signal distributed by the distribution section, and a quadrature demodulation section that frequency-multiplies a signal component corresponding to the pilot signal extracted by the extraction section by the other signal with a delay added thereto by the delay addition section and carries out quadrature demodulation.

[0030] The radio transmission apparatus of the present

invention is a radio transmission apparatus that transmits a multiplexed signal which multiplexes a modulated signal without the signal being carried on a center frequency and a pilot signal having a center
5 frequency identical to the center frequency, which adopts a configuration comprising a modulated signal generation section that generates the modulated signal, a local oscillation signal generation section that generates a local oscillation signal, a quadrature modulation section
10 that frequency-multiplies the modulated signal using the local oscillation signal generated by the local oscillation signal generation section, increases the frequency and performs quadrature modulation, a delay addition section that adds a delay to the local oscillation
15 signal generated by the local oscillation signal generation section and a combiner that multiplexes a signal after the quadrature demodulation by the quadrature demodulation section with a local oscillation signal as the pilot signal with a delay added by the delay
20 addition section so that the phases of the signals match after the quadrature demodulation.

Advantageous Effect of the Invention

[0031] According to the present invention, it is possible
25 to provide a radio system, radio transmission apparatus and radio reception apparatus which improves phase noise characteristics and thereby improves communication

quality.

Brief Description of Drawings

[0032]

5 FIG.1 is a block diagram showing the configuration of a radio system according to Embodiment 1 of the present invention;

 FIG.2 is a characteristic diagram showing frequency characteristics of each signal in the radio system;

10 FIG.3 illustrates the configuration of a quadrature modulator in the radio reception apparatus shown in FIG.1;

 FIG.4 is a block diagram showing the configuration of a radio system according to Embodiment 2 of the present invention;

15 FIG.5 is a block diagram showing the configuration of a radio system according to Embodiment 3 of the present invention;

 FIG.6 is a block diagram showing the configuration of a radio system according to Embodiment 4 of the present
20 invention;

 FIG.7 is a block diagram showing the configuration of a radio system according to Embodiment 5 of the present invention;

 FIG.8 is a block diagram showing the configuration
25 of a radio system according to Embodiment 6 of the present invention;

 FIG.9 illustrates a frequency characteristic of a

transmission signal in the radio system of FIG.8;

FIG.10 is a block diagram showing the configuration of a radio system according to Embodiment 7 of the present invention;

5 FIG.11 is a block diagram showing the configuration of a radio system according to Embodiment 8 of the present invention;

FIG.12 is a block diagram showing the configuration of a radio system according to Embodiment 9 of the present
10 invention;

FIG.13 is a block diagram showing the configuration of a radio transmission apparatus different from the configuration of the radio transmission apparatus shown in FIG.1;

15 FIG.14 is a block diagram showing the configuration of a local noise canceller provided for a conventional radio system; and

FIG.15 shows characteristic diagram illustrating frequency characteristics of the respective components
20 of the local noise canceller in FIG.14.

Best Mode for Carrying Out the Invention

[0033] With reference now to the attached drawings, embodiments of the present invention will be described
25 in detail below.

[0034] (Embodiment 1)

First of all, a radio system according to this embodiment will be explained with reference to the attached drawings.

[0035] FIG.1 is a block diagram showing the configuration of a radio system according to this embodiment. As shown in FIG.1, radio system 100 is provided with radio transmission apparatus 101 and radio reception apparatus 151.

[0036] This radio transmission apparatus 101 is provided with transmission baseband section 110 that generates a baseband signal and transmission section 120 that applies predetermined processing to the baseband signal and transmits it as an RF signal.

[0037] In this transmission baseband section 110, modulated signal generation section 111 generates a modulated signal and gives it to pilot signal combination section 112. Here, the modulated signal will be explained as multicarrier CDMA, but any type of modulated signal can be handled if it is at least not carried on a center frequency part on the frequency axis and it can be, for example, an OFDM signal.

[0038] This pilot signal combination section 112 combines the modulated signal (M-CDMA) received from modulated signal generation section 111 and a pilot signal (PILOT) received from pilot signal generation section 113 and gives the combined signal to transmission section 120.

[0039] Here, the pilot signal is positioned at the center of the modulated signal on the frequency axis and when the frequency of the pilot signal is assumed to be f_{PILOT} , $f_{\text{PILOT}}=0[\text{Hz}]$.

5 [0040] On the other hand, in transmission section 120, local oscillation section 121 generates a local oscillation signal using a reference signal generated from reference signal oscillator 122 and gives the local oscillation signal to quadrature modulator 123.

10 [0041] Quadrature modulator 123 carries out quadrature modulation on the combined signal of the modulated signal and pilot signal output from pilot signal combination section 112 of above described transmission baseband section 110 using the local oscillation signal from local
15 oscillation section 121 and gives the quadrature-modulated signal to multiplier 124.

[0042] Multiplier 124 converts the signal quadrature-modulated by quadrature modulator 123 to a radio signal using a local oscillation signal received
20 from local oscillation section 125. This radio signal is amplified by amplifier 126 and transmitted through antenna 127. Here, local oscillation section 125 generates a local oscillation signal using a reference signal generated from reference signal oscillator 122
25 and the local oscillation signals generated by local oscillation section 121 and local oscillation section 125 are synchronized with each other.

[0043] On the other hand, antenna 152 of radio reception apparatus 151 receives the radio signal transmitted from radio transmission apparatus 101. This received radio signal is amplified by amplifier 153 and then given to multiplier 154.

[0044] Multiplier 154 converts the frequency of the radio signal amplified by amplifier 153 using a local oscillation signal generated from local oscillation section 155 and gives the signal to band pass filter 156.

10 Local oscillation section 155 oscillates a local oscillation signal using a reference signal generated from reference signal oscillator 157.

[0045] Band pass filter 156 extracts only a signal of a desired frequency band from the signal frequency-converted by multiplier 154. The signal extracted by band pass filter 156 is amplified by amplifier 158 and then given to distributor 159.

[0046] Distributor 159 distributes the signal received from band pass filter 156 through amplifier 158 into two routes of a modulated signal branch and a pilot branch.

[0047] In the pilot branch, band pass filter 160 extracts only a pilot signal component from the signal distributed by distributor 159. This extracted pilot signal component is amplified by amplifier 161 and then given to quadrature demodulator 163. Here, attempting to keep the input signal level for quadrature demodulator 163 through only the pilot branch, that is, only amplifier

161 causes distortion only in the pilot branch and causes phase noise to remain in the output of quadrature demodulator 163. Thus, if it is assumed that the input signal level for distributor 159 is $P_{in}[dBm]$, power loss
5 by distributor 159 is $\alpha[dB]$, power loss of band pass filter 160 is $\beta[dB]$ and the gain of amplifier 161 is $\gamma[dB]$, then input signal level P_{in} for distributor 159 is set so that it is substantially proportional to the output level $(P_{in} + \gamma - \alpha - \beta)$ of amplifier 161. Such a setting can prevent
10 distortion in the pilot branch.

[0048] On the other hand, in the modulated signal branch, delay compensator 162 causes the signal received from distributor 159 to delay so as to be synchronized with the signal which arrives at quadrature demodulator 163
15 through the pilot branch and gives it to quadrature demodulator 163.

[0049] Quadrature demodulator 163 performs multiplication between the signals received from the pilot branch and the modulated signal branch, performs
20 quadrature demodulation on the multiplication result and gives it to reception baseband section 164.

[0050] Next, the operation of radio system 100 will be explained with reference to FIG.1 and FIG.2.

[0051] FIG.2 shows characteristic diagrams illustrating
25 a frequency characteristic of each signal at radio system 100. FIGs.2A to 2G show frequency characteristics of signals assigned corresponding letters of the alphabet

in FIG.1.

[0052] Combined signal A of the modulated signal and pilot signal output from baseband section 110 has a frequency characteristic shown in FIG.2A. As described
5 above, here the pilot signal is positioned at the center of the modulated signal on the frequency axis and if the frequency of the pilot signal is assumed to be f_{PILOT} , $f_{PILOT}=0$ [Hz].

[0053] Combined signal A is frequency-converted to a
10 radio signal and output from antenna 127.

[0054] Radio frequency f_{RF} of the modulated signal and radio frequency f_{RF_PILOT} of the pilot signal included in the radio signal output from antenna 127 are expressed as follows:

15
$$f_{RF}=f_{CDMA}+f_{Lo1}+f_{Lo2}$$

$$f_{RF_PILOT}=f_{PILOT}+f_{Lo1}+f_{Lo2}$$

[0055] Here, suppose the frequency of the modulated signal generated by modulated signal generation section 111 is f_{CDMA} , the frequency of the local oscillation signal
20 oscillated by local oscillation section 125 is f_{Lo1} , and the frequency of the local oscillation signal oscillated by local oscillation section 121 is f_{Lo2} .

[0056] Here, in transmission section 120, phase noise of local oscillation section 121 at quadrature modulator
25 123 and phase noise of local oscillation section 125 at multiplier 124 are superimposed on combined signal A and the signal is output as a radio signal. Furthermore,

phase noise is also superimposed on the radio signal in a transmission path after the signal is output from antenna 127 until it is received by antenna 152.

[0057] Therefore, if the sum total of phase noise superimposed in transmission section 120 and transmission path is $\theta(t)$, radio signal B received by antenna 152 has a frequency characteristic shown in FIG.2B and is expressed as follows:

$$f_{RF} \angle \theta(t)$$

10

$$f_{RF_PILOT} \angle \theta(t)$$

[0058] Radio signal B received by antenna 152 is amplified by amplifier 153 and frequency-converted by multiplier 154. Here, local oscillation section 155 oscillates a local signal having phase noise $\phi(t)$, and therefore this local signal has the frequency characteristic as shown in FIG.2C and is expressed as follows:

$$f_{Lo1} \angle \phi(t)$$

[0059] For this reason, phase noise $\phi(t)$ of local oscillation section 155 is superimposed on the signal frequency-converted by multiplier 154 and given to band pass filter 156.

[0060] The bandwidth of this band pass filter 156 is set in such a way that the frequencies of the difference components output from multiplier 154, that is, $f_{RF} - f_{Lo1}$ and $f_{RF_PILOT} - f_{Lo1}$ are extracted. For this reason, signal D output from amplifier 158 has a frequency characteristic

shown in FIG.2D and is expressed as follows:

$$f_{RF}-f_{Lo1} \angle \theta(t)-\varphi(t)$$

$$f_{RF_PILOT}-f_{Lo1} \angle \theta(t)-\varphi(t)$$

[0061] Next, signal D is distributed by distributor 159,
5 one is output to the modulated signal branch and the other
is output to the pilot branch.

[0062] In the pilot branch, band pass filter 156 is set
so as to extract only the pilot signal component, and
therefore band pass filter 156 extracts only the pilot
10 signal component from distributed signal D and outputs
the pilot signal component.

[0063] At this time, delay τ_1 is superimposed on signal
D when the pilot signal component passes through band
pass filter 160 and amplifier 161. For this reason,
15 output signal E of amplifier 161 has a frequency
characteristic as shown in FIG.2E and is expressed as
follows:

$$f_{RF_PILOT}-f_{Lo1} \angle \theta(t-\tau_1)-\varphi(t-\tau_1)$$

[0064] On the other hand, in the modulated signal branch,
20 such a delay as $\Delta t=\tau_1+\tau_2$ is superimposed on signal D by
delay compensator 162. Note that τ_2 is a delay generated
in quadrature demodulator 163, which will be described
later. For this reason, signal F output from delay
compensator 162 has a frequency characteristic as shown
25 in FIG.2F and can be expressed by the following expression:

$$f_{RF}-f_{Lo1} \angle \theta(t-\Delta t)-\varphi(t-\Delta t)$$

[0065] Signal E is multiplied by signal F at quadrature

demodulator 163 and then subjected to quadrature demodulation. More specifically, this quadrature demodulator 163 includes delay compensator 171, 90-degree phase shifter 172, multiplier 173 and multiplier 174 as shown in FIG.3.

[0066] Signal E is input to delay compensator 171 and 90-degree phase shifter 172. 90-degree phase shifter 172 shifts the phase of signal E by 90 degrees and outputs the signal to multiplier 174. At this time, delay τ_2 is generated at 90-degree phase shifter 172.

[0067] Delay compensator 171 compensates signal E so as to produce delay τ_2 which is equivalent to the delay generated by 90-degree phase shifter 172.

[0068] Signal F is input to multiplier 173 and multiplier 174, multiplied by the output signals from delay compensator 171 and 90-degree phase shifter 172 respectively and output as signal G. This signal F has also been compensated at delay compensator 162 with amount of delay τ_2 in quadrature demodulator 163 taken into consideration, and therefore the signals multiplied at multiplier 173 and multiplier 174 have an identical phase. It is thereby possible to realize ideal demodulation.

[0069] Therefore, signal G output from quadrature demodulator 163 has a frequency characteristic as shown in FIG.2G and can be expressed by the following expression:

$$(f_{RF} - f_{Lo1}) - (f_{RF_PILOT} - f_{Lo1})$$

$$\angle \theta(t - \tau_1 - \tau_2) - \phi(t - \tau_1 - \tau_2) - \{ \theta(t - \Delta t) - \phi(t - \Delta t) \}$$

[0070] This is organized using a condition $f_{\text{PILOT}}=0$ Hz and $\Delta t=\tau_1+\tau_2$ as follows:

$$f_{\text{CDMA}} \angle 0$$

[0071] This means that phase noise superimposed at
5 transmission section 120, transmission path and local
oscillation section 155 has been completely canceled and
the modulated signal generated at modulated signal
generation section 111 has been demodulated at radio
reception apparatus 151. That is, it is possible to
10 cancel not only phase noise superimposed on the received
signal but also phase noise generated in the system of
the reception radio section.

[0072] As described above, radio transmission apparatus
101 transmits a signal multiplexed in such a way that
15 a pilot signal is carried on the center frequency of the
transmission signal, radio reception apparatus 151
performs frequency multiplication using a pilot signal
having the same frequency error and phase noise as those
of the received signal and also performs frequency
20 multiplication on phase noise generated in the system
using a signal having the same phase noise. For this
reason, it is possible to remove frequency errors and
phase errors included in the received signal and also
completely remove phase errors generated in the system
25 and thereby realize a radio system having an excellent
phase noise characteristic.

[0073] When band pass filter 160 extracts a pilot signal,

it cannot extract phase noise outside the frequency band of band pass filter 160, and therefore the phase noise is included in the frequency characteristic shown in FIG.2G. However, this phase noise can be suppressed by
5 local oscillation section 121, local oscillation section 125 and local oscillation section 155.

[0074] For example, local oscillation section 155 is constructed as a PLL frequency synthesizer and the loop bandwidth is designed to be not greater than the bandwidth
10 of band pass filter 160. By so doing, it is possible to suppress phase noise $\phi(t)$ outside the pass band of band pass filter 160 shown in FIG.2C and thereby ignore influences thereof. Note that local oscillation section 121 and local oscillation section 125 can also suppress
15 phase noise $\theta(t)$ outside the frequency band of band pass filter 160 in the same way.

[0075] Furthermore, in this embodiment, a signal having the same frequency (f_{L01}) as that of the local oscillation signal oscillated by local oscillation section 125 at
20 radio transmission apparatus 101 is used as a local frequency oscillated by local oscillation section 155 of radio reception apparatus 151, but the signal only needs to have a frequency which does not exceed $2 \times RF$ frequency ($f_{L01} + f_{L02}$) and is different from the RF
25 frequency, and it goes without saying that it is likewise possible to cancel phase noise using the same frequency (f_{L02}) as the local oscillation signal oscillated by local

oscillation section 121.

[0076] Furthermore, this embodiment assumes that the configurations of transmission baseband section 110 and transmission section 120 are based on a superheterodyne
5 scheme, but any scheme can be used if it is at least a scheme capable of transmitting a signal having the frequency characteristic shown in FIG.2A with a pilot signal disposed at the center of a modulated signal on the frequency axis and can be, for example, direct
10 conversion.

[0077] In this way, according to Embodiment 1, radio reception apparatus 151 is provided with antenna 152 that receives a radio signal in which a modulated signal without the signal being carried on the center frequency is
15 multiplexed with a pilot signal having a center frequency identical to the center frequency thereof, distributor 159 that distributes the received signal received from antenna 152 into two directions, band pass filter 160 that extracts from the one received signal distributed
20 from distributor 159 a signal component corresponding to the pilot signal having a center frequency identical to the center frequency thereof, delay compensator 162 that gives a delay to the other signal distributed by distributor 159 and quadrature demodulator 163 that
25 frequency-multiplies the signal component corresponding to the pilot signal extracted by band pass filter 160 by the other signal with a delay added by delay compensator

162 and also performs quadrature demodulation.

[0078] By so doing, the radio signal received is a modulated signal with the signal not being carried on a center frequency multiplexed with a pilot signal having
5 a center frequency identical to the above described center frequency, which eliminates the necessity for local oscillation section 60 and frequency converter 61 existing in the signal branch of the local noise canceller shown in the conventional example, and therefore phase
10 noise included in a local oscillation signal generated at this local oscillation section 60 is not carried on a signal (signal F) of the signal branch. For this reason, it is also possible to completely remove phase errors generated in the system and thereby realize a radio system
15 having an excellent phase noise characteristic.

[0079] Furthermore, above described quadrature demodulator 163 is provided with 90-degree phase shifter 172 that applies a phase shift of 90 degrees to a signal component corresponding to a pilot signal extracted by
20 band pass filter 160, multiplier 174 that multiplies the signal (signal E) with a delay added thereto by delay compensator 162 by a signal component corresponding to a pilot signal to which a phase shift of 90 degrees is applied, multiplier 173 that multiplies the signal
25 (signal E) with a delay added thereto by delay compensator 162 by a signal component corresponding to the pilot signal extracted by band pass filter 160 and delay compensator

171 that adds a delay equivalent to the delay generated by 90-degree phase shifter 172 to the signal component corresponding to the pilot signal multiplied at multiplier 173.

5 [0080] By so doing, delay compensator 162 sets an amount of delay to be added appropriately, and it is thereby possible to match the phases of signals multiplied at multiplier 173 and multiplier 174.

10 [0081] (Embodiment 2)

FIG.4 is a block diagram showing the configuration of a radio system according to Embodiment 2 of the present invention. Compared to radio reception apparatus 151 of radio system 100 according to Embodiment 1, radio
15 reception apparatus 351 of radio system 300 shown in FIG.4 only differs in that amplifier 352 is added between distributor 159 and band pass filter 160 and the rest of the components are the same. Therefore, explanations of the same components will be omitted and only different
20 parts will be explained below.

[0082] Noting that when a comparison is made between a modulated signal branch and a pilot signal branch, the pilot signal branch is inferior to the modulated signal branch in an NF characteristic and C/N characteristic
25 when the electric field is weak because the pilot signal branch includes band pass filter 160, this embodiment has added amplifier 352 between distributor 159 and band

pass filter 160 in radio reception apparatus 351.

[0083] In the pilot branch of radio reception apparatus 351, amplifier 352 amplifies signal D distributed by distributor 159 and gives the amplified signal to band
5 pass filter 160.

[0084] Band pass filter 160 extracts only a pilot signal component from the signal amplified by amplifier 352. This extracted pilot signal component is amplified by amplifier 161 and then given to quadrature demodulator
10 163.

[0085] As described above, adding amplifier 352 before band pass filter 160 makes it possible to improve the NF characteristic and C/N characteristic of the pilot branch when the electric field is weak.

15 [0086] It is possible to use a directional coupler or the like to improve the isolation characteristic of distributor 159. Adding amplifier 352 between distributor 159 and band pass filter 160 makes it possible to improve the NF characteristic of the pilot branch and
20 C/N characteristic when the electric field is weak in this case, too.

[0087] As described above, it is possible to realize a radio system having an excellent NF characteristic of the pilot branch and C/N characteristic when the electric
25 field is weak, and an excellent phase noise characteristic.

[0088] In this way, according to Embodiment 2, radio

reception apparatus 351 is provided with antenna 152 that receives a radio signal in which a modulated signal without the signal being carried on the center frequency is multiplexed with a pilot signal having a center frequency identical to the center frequency, distributor 159 that distributes the received signal received from antenna 152 into two directions, bandpass filter 160 that extracts from the one received signal distributed from distributor 159 a signal component corresponding to the pilot signal having a center frequency identical to the center frequency thereof, delay compensator 162 that gives a delay to the other signal distributed by distributor 159, and quadrature demodulator 163 that frequency-multiplies the signal component corresponding to the pilot signal extracted by band pass filter 160 by the other signal with a delay added by delay compensator 162 and also performs quadrature demodulation.

[0089] Furthermore, radio reception apparatus 351 is provided with amplifier 352 that amplifies the signal (signal for the pilot branch) distributed by distributor 159 and outputs the signal to band pass filter 160.

[0090] By so doing, it is possible to improve the NF characteristic and the C/N characteristic when the electric field is weak of the signal (signal E) input to quadrature demodulator 163 through the pilot branch, and thereby further improve the phase noise characteristic.

[0091] (Embodiment 3)

FIG.5 is a block diagram showing the configuration of a radio system according to this Embodiment 3. Compared to radio reception apparatus 151 of radio system 100 in Embodiment 1, radio reception apparatus 451 of radio system 400 shown in FIG.5 only differs in that variable gain amplifier 452 is added instead of amplifier 158 and reception baseband section 164 is replaced by reception baseband section 454 provided with reception power calculation section 453 and the rest of the components are the same. Therefore, explanations of the same components will be omitted and only different parts will be explained below.

[0092] Here, when power received by antenna 152 fluctuates, power input to amplifier 161 fluctuates. When a delay generated in the pilot branch fluctuates, the delay value of delay compensator 162 cannot be uniquely determined. Noting such a point, this embodiment adds variable gain amplifier 452 instead of amplifier 158 and provides reception baseband section 454 equipped with reception power calculation section 453 instead of reception baseband section 164.

[0093] This reception power calculation section 453 calculates power of received signal B from power of signal G output from quadrature demodulator 163. Reception baseband section 454 gives a control signal corresponding

to this calculation result to variable gain amplifier 452 and controls the gain thereof. This makes it possible to keep constant power input to distributor 159, and as a result, make constant the delay generated in the pilot
5 branch and thereby uniquely determine the delay value of delay compensator 162.

[0094] As described above, it is possible to realize a radio system having an excellent phase noise characteristic even when the reception power changes.

10 [0095] In this way, according to Embodiment 3, radio reception apparatus 451 is provided with antenna 152 that receives a radio signal in which a modulated signal without the signal being carried on the center frequency is multiplexed with a pilot signal having a center frequency
15 identical to the center frequency, distributor 159 that distributes the received signal received from antenna 152 into two directions, bandpass filter 160 that extracts from the one received signal distributed from distributor 159 a signal component corresponding to the pilot signal
20 having a center frequency identical to the center frequency thereof, delay compensator 162 that gives a delay to the other signal distributed by distributor 159, and quadrature demodulator 163 that frequency-multiplies the signal component corresponding to the pilot signal
25 extracted by band pass filter 160 by the other signal with a delay added by delay compensator 162 and also performs quadrature demodulation.

[0096] Furthermore, radio reception apparatus 451 is provided with reception power calculation section 453 that calculates a reception power value of the received signal based on the amplitude of the output signal of quadrature demodulator 163 and variable gain amplifier 452 that is disposed before distributor 159 and amplifies the received signal according to the calculated reception power value.

[0097] By so doing, even when the reception power received by antenna 152 fluctuates, it is possible to realize amplification according to the reception power value, keep constant the power input to distributor 159 and as a result keep constant the delay generated in the pilot branch. Therefore, it is possible to prevent deterioration of the phase noise characteristic even when the reception power fluctuates.

[0098] (Embodiment 4)

FIG.6 is a block diagram showing the configuration of a radio system according to this Embodiment 4. Compared to radio reception apparatus 451 of radio system 400 in Embodiment 3, radio reception apparatus 551 of radio system 500 shown in FIG.6 only differs in that amplifier 153 is replaced by variable gain amplifier 552 and reception baseband section 454 is replaced by reception baseband section 554 and the rest of the components are the same. Therefore, explanations of the

same components will be omitted and only different parts will be explained below.

[0099] Reception baseband section 554 receives signal G from quadrature demodulator 163 and reception power calculation section 453 calculates power of received signal B from the power of signal G. Reception baseband section 554 then gives control signals according to this calculation result to variable gain amplifier 552 and variable gain amplifier 452 and controls those gains.

10 [0100] By so doing, when the variable gain width of variable gain amplifier 452 is set to G_1 dB and the variable gain width of variable gain amplifier 552 is set to G_2 dB, the variable gain width of the entire system becomes (G_1+G_2) dB and it is possible to respond to fluctuations in the reception level with a further wider range.

[0101] As described above, even when the reception power fluctuates over a wide range, it is possible to realize a radio system with an excellent phase noise characteristic.

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[0102] (Embodiment 5)

FIG.7 is a block diagram showing the configuration of a radio system according to Embodiment 5. Compared to radio reception apparatus 451 of radio system 400 in Embodiment 3, radio reception apparatus 651 of radio system 600 shown in FIG.7 only differs in that temperature sensor section 652 is provided, reception baseband

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section 454 is replaced by reception baseband section 654 provided with reception power calculation section 453 and temperature/delay deviation calculation section 653 and delay compensator 162 is replaced by delay compensator 655, and the rest of the components are the same. Therefore, explanations of the same components will be omitted and only different parts will be explained below.

[0103] Noting that a delay variation according to temperature at amplifier 161 becomes an error when phase noise is canceled, this embodiment provides temperature sensor section 652, temperature/delay deviation calculation section 653 and delay compensator 655.

[0104] Reception baseband section 654 stores measured values of delay deviation with respect to the temperature of amplifier 161.

[0105] Temperature/delay deviation calculation section 653 provided for this reception baseband section 654 calculates a delay deviation based on temperature data measured by temperature sensor section 652. Reception baseband section 654 gives a control signal according to this calculation result to delay compensator 655 and controls the delay value of delay compensator 655.

[0106] Here, the case where radio reception apparatus 451 of Embodiment 3 is provided with temperature sensor section 652, temperature/delay deviation calculation section 653 and delay compensator 655 has been explained,

but this is also applicable to any one of Embodiments 1 to 4.

[0107] As described above, even when the delay of the amplifier fluctuates depending on the temperature, it is possible to realize a radio system with an excellent phase noise characteristic.

[0108] In this way, according to Embodiment 5, radio reception apparatus 651 is provided with antenna 152 that receives a radio signal in which a modulated signal without the signal being carried on the center frequency is multiplexed with a pilot signal having a center frequency identical to the center frequency, distributor 159 that distributes the received signal received from antenna 152 into two directions, band pass filter 160 that extracts from the one received signal distributed from distributor 159 a signal component corresponding to the pilot signal having a center frequency identical to the center frequency thereof, delay compensator 162 that gives a delay to the other signal distributed by distributor 159, and quadrature demodulator 163 that frequency-multiplies the signal component corresponding to the pilot signal extracted by band pass filter 160 by the other signal with a delay added by delay compensator 162 and also performs quadrature demodulation.

[0109] Furthermore, radio reception apparatus 651 is provided with temperature sensor section 652 that measures a temperature and temperature/delay deviation

calculation section 653 that calculates an amount of delay based on the temperature and delay compensator 655 changes the delay to be added based on the calculated amount of delay.

5 [0110] By so doing, even when the delay of the amplifier in the pilot branch fluctuates according to the temperature, delay compensator 655 can compensate for the delay according to the delay variation, and therefore it is possible to match the phases of input signals for
10 quadrature demodulator 163 and thereby improve the phase noise characteristic.

[0111] (Embodiment 6)

FIG.8 is a block diagram showing the configuration
15 of a radio system according to this Embodiment 6. Compared to radio reception apparatus 151 of radio system 100 according to Embodiment 1, radio reception apparatus 751 of radio system 700 shown in FIG.8 only differs in that quadrature demodulator 163 is replaced by multiplier
20 752 and reception baseband section 164 is replaced by reception baseband section 753, and the rest of the components are the same. Furthermore, this embodiment differs only in that a pilot signal superimposed on a transmission signal is multiplexed in the vicinity of
25 the center of a modulated signal, that is, on a frequency shifted by Δf from the center as shown in FIG.9. Therefore, explanations of the same components will be omitted and

only different parts will be explained below.

[0112] Multiplier 752 multiplies signal E amplified by amplifier 161 and signal F with a delay added thereto by delay compensator 162 and outputs the multiplication
 5 result to reception baseband section 753. Band pass filter 160 is adjusted so as to extract a pilot signal component having a frequency shifted by Δf from the above described center from the signal distributed by distributor 159.

10 [0113] Here, signal G output from multiplier 752 can be expressed as follows:

$$\begin{aligned} & (f_{RF} - f_{LO1}) - (f_{RF_PILOT} - f_{LO1}) \\ & = (f_{RF} - f_{LO1}) - (f_{RF} - \Delta f - f_{LO1}) \angle \\ & \theta(t - \tau_1 - \tau_2) - \varphi(t - \tau_1 - \tau_2) - \{ \theta(t - \Delta t) - \Delta\theta(t - \Delta t) - \varphi(t - \Delta t) \} \end{aligned}$$

15 [0114] This is organized using a condition of $f_{PILOT} = 0$ Hz and $\Delta t = \tau_1 + \tau_2$ as follows:

$$f_{CDMA} + \Delta f \angle \Delta\theta(t - \Delta t)$$

[0115] Reception baseband section 753 applies predetermined processing to the output signal of this
 20 multiplier 752 and obtains a baseband signal.

[0116] Here, when the frequency of Δf is set to a frequency lower than the RF frequency and IF frequency, phase noise $\Delta\theta(t - \Delta t)$ becomes a very small value, and therefore there is substantially no influence on the reception
 25 characteristic of reception baseband section 753. For this reason, this embodiment is suitably applicable to a Low-IF scheme or the like whereby demodulation is

performed using a low frequency signal.

[0117] Thus, adopting the configuration of multiplexing a pilot signal to be superimposed on the transmission signal with the modulated signal in the vicinity of the center thereof and using multiplier 752 instead of quadrature demodulator 163 makes it possible to support a reception scheme such as a Low-IF scheme. It is also possible to realize a radio system having an excellent phase noise characteristic. This configuration is also applicable to each radio reception apparatus of the radio system of Embodiment 2 to Embodiment 5.

[0118] (Embodiment 7)

FIG.10 is a block diagram showing the configuration of a radio system according to this Embodiment 7. Compared to radio reception apparatus 151 of radio system 100 according to Embodiment 1, radio reception apparatus 851 of radio system 800 shown in FIG.10 only differs in that reception baseband section 164 is replaced by reception baseband section 853 provided with filter bandwidth control section 852, band pass filter 160 is replaced by bandwidth variable band pass filter 854 and local oscillation section 155 is replaced by PLL frequency synthesizer 855, and the rest of the components are the same. Therefore, explanations of the same components will be omitted and only different parts will be explained below.

[0119] Filter bandwidth control section 852 controls the bandwidth of bandwidth variable band pass filter 854 by giving a signal to control the bandwidth.

[0120] In this way, even when the distance between the
5 frequency of the modulated signal and the frequency of the pilot signal is changed, it is possible to extract the pilot signal by controlling the bandwidth of bandwidth variable band pass filter 854 using filter bandwidth control section 852.

10 [0121] However, since it is not possible to extract phase noise outside the frequency band of bandwidth variable band pass filter 854, the phase noise suppression characteristic deteriorates.

[0122] Thus, if local oscillation section 155 is replaced
15 by PLL frequency synthesizer 855, filter bandwidth control section 852 controls the loop bandwidth of PLL frequency synthesizer 855 and the loop bandwidth is set to or below the bandwidth of bandwidth variable band pass filter 854, it is possible to suppress phase noise within
20 the band of bandwidth variable band pass filter 854.

[0123] In this way, by controlling the bandwidth of bandwidth variable band pass filter 854 and the loop bandwidth of PLL frequency synthesizer 855, it is possible to suppress influences of phase noise outside the
25 bandwidth variable band pass filter 854. This configuration is also applicable to the radio reception apparatus in the radio system according to Embodiment

2 to Embodiment 6.

[0124] Thus, even when the distance between the frequency of the modulated signal and the frequency of the pilot signal is changed, it is possible to realize a radio system
5 having an excellent phase noise characteristic. Furthermore, by adopting such a configuration for the radio system of the present invention, the present invention is also applicable to a plurality of communication systems having different distances between
10 the frequency of the modulated signal and frequency of the pilot signal.

[0125] In this way, according to Embodiment 7, radio reception apparatus 851 is provided with antenna 152 that receives a radio signal in which a modulated signal without
15 the signal being carried on the center frequency is multiplexed with a pilot signal having a center frequency identical to the center frequency, distributor 159 that distributes the received signal received from antenna 152 into two directions, band pass filter 160 that extracts
20 from the one received signal distributed from distributor 159 a signal component corresponding to the pilot signal having a center frequency identical to the center frequency thereof, delay compensator 162 that gives a delay to the other signal distributed by distributor 159,
25 and quadrature demodulator 163 that frequency-multiplies the signal component corresponding to the pilot signal extracted by band pass filter 160 by the other signal

with a delay added by delay compensator 162 and also performs quadrature demodulation.

[0126] Furthermore, a superheterodyne scheme is applied to radio reception apparatus 851 and radio reception
5 apparatus 851 is provided with filter bandwidth control section 852 that generates a control signal for controlling the filter bandwidth, PLL frequency synthesizer 855 that controls and oscillates the bandwidth of a local oscillation signal based on the
10 control signal and multiplier 154 that is disposed before distributor 159 and frequency-multiplies the received signal received by antenna 152 and the local oscillation signal whose bandwidth is controlled by PLL frequency synthesizer 855, and bandwidth variable band pass filter
15 854 is made to change the bandwidth to be extracted based on the above described control signal.

[0127] By so doing, it is possible to suppress influences of phase noise outside the bandwidth of bandwidth variable band pass filter 854 by controlling the bandwidth of
20 bandwidth variable band pass filter 854 and loop bandwidth of PLL frequency synthesizer 855 and improve the phase noise characteristic. Furthermore, this embodiment is also applicable to the case where signals with a different distance between the frequency of the modulated signal
25 and the frequency of the pilot signal are received.

[0128] (Embodiment 8)

FIG.11 is a block diagram showing the configuration of a radio system according to this Embodiment 8. Compared to radio reception apparatus 451 of radio system 400 according to Embodiment 3, radio reception apparatus 951 of radio system 900 shown in FIG.11 only differs in that variable gain amplifier 952 and variable gain amplifier 953 are added after quadrature demodulator 163 and reception baseband section 454 is replaced by reception baseband section 954, and the rest of the components are the same. Therefore, explanations of the same components will be omitted and only different parts will be explained below.

[0129] Reception baseband section 954 receives signal G from quadrature demodulator 163 and reception power calculation section 453 calculates power of signal G. Reception baseband section 954 gives control signals according to this calculation result to variable gain amplifier 952 and variable gain amplifier 953 and controls those gains.

[0130] By so doing, when the variable gain width of variable gain amplifier 452 is set to $G1$ dB and the variable gain width of variable gain amplifier 952 and variable gain width of variable gain amplifier 953 are set to $G3$ dB, the variable gain width of the entire system becomes $(G1+G3)$ dB and it is possible to cover fluctuations in the reception level over a further wider range.

[0131] This embodiment has explained the case where

variable gain amplifier 952 and variable gain amplifier 953 are added after quadrature demodulator 163 of Embodiment 3, but the embodiment is also applicable to any of Embodiment 4 and Embodiment 5.

5 [0132] In this way, according to Embodiment 8, radio reception apparatus 951 is provided with antenna 152 that receives a radio signal in which a modulated signal without the signal being carried on the center frequency is multiplexed with a pilot signal having a center frequency
10 identical to the center frequency, distributor 159 that distributes the received signal received from antenna 152 into two directions, bandpass filter 160 that extracts from the one received signal distributed from distributor 159 a signal component corresponding to the pilot signal
15 having a center frequency identical to the center frequency thereof, delay compensator 162 that gives a delay to the other signal distributed by distributor 159, and quadrature demodulator 163 that frequency-multiplies the signal component corresponding to the pilot signal
20 extracted by band pass filter 160 by the other signal with a delay added by delay compensator 162 and also performs quadrature demodulation.

[0133] Furthermore, radio reception apparatus 951 is provided with reception power calculation section 453
25 that calculates a reception power value of the received signal based on the amplitude of an output signal of quadrature demodulator 163, and variable gain amplifier

952 and variable gain amplifier 953 that amplify the signal subjected to quadrature demodulation by quadrature demodulator 163 according to the calculated reception power value.

5 [0134] By so doing, even when the reception power fluctuates over a wide range, it is possible to prevent deterioration of the phase noise characteristic.

[0135] (Embodiment 9)

10 FIG.12 is block diagram showing the configuration of a radio system according to Embodiment 9. Compared to radio reception apparatus 151 according to Embodiment 1, radio reception apparatus 1051 of radio system 1000 shown in FIG.12 differs in that band limiting filter 1052
15 is provided after distributor 159, and the rest of the components are the same. Therefore, explanations of the same components will be omitted and only different parts will be explained below.

[0136] Here, when a pilot signal component is carried
20 on a center frequency as in the case of signal D, DC offset may have occurred and there is a possibility that the reception characteristic may deteriorate.

[0137] Thus, band limiting filter 1052 is set so as to remove only a pilot signal component from the signal
25 received from distributor 159. For this reason, signal F which is the output signal from delay compensator 162 in this embodiment has no peak corresponding to a pilot

signal component in the center frequency area.

[0138] Quadrature demodulator 163 then multiplies
signal F deprived of the peak corresponding to the pilot
signal component in the center frequency area by signal
5 E, then performs quadrature demodulation and gives the
signal to reception baseband section 164. By so doing,
a peak corresponding to the pilot signal component in
the center frequency area in the signal input to quadrature
demodulator 163 is removed by band limiting filter 1052
10 in the modulated signal branch, and it is thereby possible
to remove influences of a DC offset in the signal input
to quadrature demodulator 163. For this reason, it is
possible to prevent distortion from occurring in the
signal input from quadrature demodulator 163 to reception
15 baseband section 164 and thereby improve the reception
characteristic. That is, by preventing distortion
caused by a DC offset from occurring, it is possible to
improve the reception characteristic.

[0139] In this way, according to Embodiment 9, radio
20 reception apparatus 1051 is provided with antenna 152
that receives a radio signal in which a modulated signal
without the signal being carried on the center frequency
is multiplexed with a pilot signal having a center
frequency identical to the center frequency, distributor
25 159 that distributes the received signal received from
antenna 152 into two directions, band pass filter 160
that extracts from the one received signal distributed

from distributor 159 a signal component corresponding to the pilot signal having a center frequency identical to the center frequency thereof, delay compensator 162 that gives a delay to the other signal distributed by distributor 159, and quadrature demodulator 163 that frequency-multiplies the signal component corresponding to the pilot signal extracted by band pass filter 160 by the other signal with a delay added by delay compensator 162 and also performs quadrature demodulation.

10 [0140] Furthermore, radio reception apparatus 1051 is provided with band limiting filter 1052 that is disposed before delay compensator 162 and removes a signal component corresponding to a pilot signal having a center frequency identical to the center frequency of the signal distributed by distributor 159 from the signal.

15 [0141] This removes a peak corresponding to the pilot signal component in the center frequency area of the signal input from band limiting filter 1052 to quadrature demodulator 163, and can thereby remove influences of a DC offset in the signal input to quadrature demodulator 163. For this reason, it is possible to prevent distortion from occurring in the signal input from quadrature demodulator 163 to reception baseband section 164 and thereby improve the reception characteristic.

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[0142] (Embodiment 10)

This embodiment relates to a radio transmission

apparatus having a configuration different from that of radio transmission apparatus 101 according to Embodiment 1 to Embodiment 9. Transmission baseband section 110 of radio communication apparatus 101 multiplexes a pilot
5 signal so as to be positioned at the center of the modulated signal on the frequency axis, and therefore there is a possibility that a DC offset may have occurred in the signal input from transmission baseband section 110 to quadrature modulator 123 and the reception characteristic
10 on the receiving side may deteriorate because of this. Therefore, this embodiment causes a pilot to be carried on the signal after quadrature modulation at the center of the frequency axis. Furthermore, a local oscillation signal is used as this pilot signal.

15 [0143] As shown in FIG.13, radio transmission apparatus 1101 according to this embodiment is provided with transmission baseband section 1110 that generates a baseband signal and transmission section 1120 that applies predetermined processing to the baseband signal
20 and sends it as an RF signal.

[0144] In this transmission baseband section 1110, modulated signal generation section 1111 generates a modulated signal and inputs an I component and Q component of the modulated signal to quadrature modulator 123 of
25 transmission section 1120. Here, the modulated signal will be explained as multicarrier CDMA, but any modulated signal can be handled if at least no signal is carried

on the center frequency part on the frequency axis and, for example, an OFDM signal may also be used.

[0145] Distributor 1121 distributes a local oscillation signal from local oscillation section 121 and inputs it
5 to quadrature modulator 123 and delay compensator 1122.

[0146] Delay compensator 1122 adds a delay in such a way that the time after a local oscillation signal distributed by distributor 1121 is input to quadrature modulator 123 until quadrature modulator 123 performs quadrature
10 modulation on the modulated signal using the local oscillation signal and then the signal is input to combiner 1123 becomes the same as the time until the local oscillation signal distributed by distributor 1121 is input to the combiner 1123, that is, both signals have
15 the same phase.

[0147] Combiner 1123 combines the output signal of quadrature modulator 123 and the output signal from delay compensator 1122 and inputs the combined signal to multiplier 124. At this time, the signal output from
20 combiner 1123 has a local oscillation signal (generated by local oscillation section 121) as a pilot signal on the signal after quadrature modulation at the center of the frequency axis.

[0148] Thus, according to Embodiment 10, it is possible
25 to generate and send a radio signal in which a modulated signal free of influences of a DC offset with the signal not being carried on the center frequency is multiplexed

with a pilot signal having a center frequency identical to the center frequency thereof.

[0149] (Other Embodiments)

5 (1) Radio transmission apparatus 101 and radio transmission apparatus 1101 according to Embodiment 1 to Embodiment 10 have been explained as the ones to which a superheterodyne scheme is applied. However, the present invention is not limited to this and a direct
10 conversion scheme may also be applicable thereto. In this case, radio transmission apparatus 101 and radio transmission apparatus 1101 need not be provided with multiplier 124 and local oscillation section 125 and the output signal of quadrature modulator 123 has a radio
15 frequency.

[0150]

(2) The radio reception apparatus according to Embodiment 1 to Embodiment 9 has been explained as the one to which a superheterodyne scheme is applied. However, the
20 present invention is not limited to this and a direct modulation scheme may also be applied. In this case, the radio reception apparatus according to the above described embodiments does not require multiplier 154, local oscillation section 155, band pass filter 156 and
25 reference signal oscillator 157 and the input signal for distributor 159 has a radio frequency.

[0151] The present application is based on Japanese

Patent Application No.2004-089725 filed on March 25, 2004 and Japanese Patent Application No.2005-82443 filed on March 22, 2005, entire content of which is expressly incorporated by reference herein.

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Industrial Applicability

[0152] The radio system, radio transmission apparatus and radio reception apparatus of the present invention has an effect of improving a phase noise characteristic and is useful for use in various radio communication apparatuses such as cellular phone, PHS, radio LAN and a radio system made up of these devices.

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